Anti-Windup Algorithms for Pilot-Induced-Oscillation Alleviation

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The paper deals with the development of anti-windup schemes and related numerical oriented tools. The objective is then to design anti-windup compensators to guarantee stability and performance for some particular classes of nonlinear actuators presenting both magnitude and rate saturations. The lateral flying case for a civil aircraft undergoing aggressive maneuvering by the pilot is addressed. A complete methodology including theoretical conditions and associated toolbox is then proposed and compared to solutions based on anti-PIO filters.

Introduction

The paper is aimed at developing anti-windup schemes and related numerical tools, in order to alleviate the Pilot-Induced-Oscillations in the lateral flying case for a civil aircraft undergoing aggressive maneuvering by the pilot. Indeed, anti-windup strategies represent an appropriate framework to mitigate the undesired saturation effects [24], [31]. Thus, the general principle of the anti-windup scheme can be depicted in Figure 1, where the (unconstrained) signal produced by the controller is compared to what is actually fed into the plant (the constrained signal). This difference is then used to adjust the control strategy by preserving stability and performance.

![Figure 1 – Anti-windup principle](image)

Such an anti-windup scheme is crucial for many control plants, since adding such a compensator to a previously computed control loop enables the performance of the closed-loop system to be improved, and could even prevent dramatic behavior, such as diverging solutions, when starting from bad initial conditions. For instance, [2], [3], [13], [14], [11], [12], [24] discuss several examples of open-loop unstable or stable physical systems presenting diverging solutions due to the presence of saturations. In particular, this undesirable nonlinear behavior appears for all exponentially unstable open-loop control systems, as well as for some marginally stable open-loop systems, as established in [23], [29].

Actually, this problem is particularly crucial for the space and aeronautical fields, where the Pilot-Induced-Oscillation (PIO) phenomenon is observed; that is, the existence of a particular external excitation (signal \( w \) in the notation of Figure 1) renders the closed-loop system unstable without anti-windup compensator [1], [15]. Thus, ad-hoc [22], [16] or advanced anti-windup strategies [8], [9], [18] for PIO suppression have been proposed in the literature and applied in practice.

For a given plant in closed loop with a pre-designed controller (designed without taking into account the saturation constraint) and a saturating input, the design of the anti-windup compensator is usually split into two steps, as explained in [26]. First, an analysis study is performed to estimate the effect of the isolated nonlinearity on the performance of the closed-loop system. Then, the second step is the design of an anti-windup compensator to improve the performance. By “performance”, various notions could be considered, such as the \( L_2 \) gain between a perturbation \( w \) and the regulated output \( z \), as depicted in Figure 1. Of course, this performance estimation is associated with an estimation of the region where the initial conditions need to be restricted, in order to guarantee the asymptotic or exponential stability of the origin.

Numerous methods exist for the design of anti-windup compensators for control systems in the presence of magnitude or rate saturation constraints. See, for example, [11], [30], [10], [28], [24], [31] to cite just a few books, surveys or special issues on this subject. Of course, the aim of this paper is not to give an exhaustive perspective about anti-windup compensator design, but rather to present some hints and algorithms on how to solve numerically the anti-windup compensator design problem for an application purpose. Actually, due to the classical tradeoff between performance and estimation of the suitable region of initial conditions, the design of anti-windup
compensators is cast into a static optimization problem, written in terms of Linear Matrix Inequalities (LMIs). Such an optimization problem can be solved numerically in an efficient way using classical software in a Matlab environment. To illustrate the approach and algorithms, the anti-windup compensator design methods are applied to a lateral aircraft model, in order to provide a systematic way to mitigate the PIO phenomenon. Although actuator loss is not exactly the subject of the paper, we illustrate the case where only one aileron is available, allowing us to consider a harsh limit on the actuator bounds to better exhibit the effect of saturation and anti-windup actions.

This paper is organized as follows. First, the model and the problem under consideration are stated in Section "Model description and problem formulation". The main results are presented in Section "Main anti-windup design conditions", where numerically tractable conditions are given to solve the anti-windup compensator design problem and some efficient algorithms are given. The numerical tools used to actually solve the problem are focused on in Section "Dedicated software tools for solving saturated and anti-windup problems". These tools are then illustrated through an application to a realistic model for a civil transport aircraft in Section "PIO alleviation using an anti-windup loop". Some concluding remarks and perspectives end the paper.

Model description and problem formulation

The full model, including the plant, actuator, controller and anti-windup loop, is precisely defined below.

Plant model

We assume that the output of the controller is not affected in the same way by the nonlinear elements. The vector \( u \in \mathbb{R}^m \) building the \( m \) inputs of the plant is broken down into two subvectors: the first one, denoted by \( u_s \in \mathbb{R}^{m_s} \), corresponds to \( m_s \) saturated inputs, whereas the second one, denoted by \( u_{ns} \in \mathbb{R}^{m_{ns}} \), corresponds to the linear inputs (unsaturated inputs). The plant model can be defined by:

\[
\begin{align*}
\text{sysP} : & \quad \dot{x} = A_p x + B_p u_s + B_{ns} u_{ns} + B_{ps} w \\
y_s &= C_p x + D_p u_s + D_{ps} u_{ns} + D_{ps} w \\
z &= C x + D u_s + D_{ns} u_{ns} + D_{ns} w
\end{align*}
\]

where \( x_p \in \mathbb{R}^{n_p} \) and \( w \in \mathbb{R}^n \) are the state and the measured output of the plant. \( w \in \mathbb{R}^n \) generally represents an exogenous perturbation, but may also be used to represent a reference signal (or both). Furthermore, \( z \in \mathbb{R}^n \) represents the regulated output, which is used to evaluate the performance of the system with respect to the perturbation \( w \) via some appropriate optimization criteria.

Controller model

Unlike the classical anti-windup loops, in which the output of the anti-windup controller is injected into the dynamics of the controller and/or the output of the controller, we consider here that the output of the anti-windup controller modifies only partially the dynamics of the controller and/or the output of the controller. Thus, the dynamical controller is described as follows:

\[
\begin{align*}
\text{sysC} : & \quad \dot{x}_c = A_c x_c + B_c u_c + B_{cs} w + B_{vc} v_c \\
y &= C_c x_c + D_c u_c + D_{cs} w + D_{vc} v_c \\
y_{ns} &= C_{ns} x_c + D_{ns} u_c + D_{ns} w
\end{align*}
\]

where \( x_c \in \mathbb{R}^{n_c} \) and \( u \in \mathbb{R}^r \) are the state and the input of the controller. The output of the controller is broken down into two signals: \( y_{ns} \in \mathbb{R}^{n_{ns}} \), which will be interconnected with a saturated actuator, and \( y_{cs} \in \mathbb{R}^{n_{cs}} \), which will be interconnected with the linear (unsaturated) input \( u_{ns} \). Moreover, \( v_c \) and \( v_s \) are the additional inputs that will be connected to the anti-windup controller. \( B_{cs} \) and \( D_{cs} \) are matrices of dimensions \( n_s \times n_c \) and \( m_s \times m_s \), and make it possible to specify what the \( n_c \) states and \( m_s \) outputs modified by the anti-windup action are.

Actuator model

The actuator block between the output of the controller \( y_s \) and the input of the plant \( u \) is divided into two blocks: the first one corresponding to the nonlinear (saturated) part and the second one corresponding to the linear (unsaturated) part. The nonlinear actuator part involves \( n_{cr} \) nested saturations, including the case of rate and magnitude saturations, as depicted in Figure 2(a). Such nonlinearities are tackled via the use of dead-zone, denoted by \( \phi_i() \), \( i = 1, ..., n_{cr} \).

\[
\begin{align*}
(a) & \quad y_{cr} = \begin{cases} u & \text{if } |u| \leq \delta_i \\
\pm \delta_i & \text{otherwise} \end{cases} \\
(b) & \quad y_{cs} = \begin{cases} u & \text{if } |u| \leq \delta_i \\
\pm \delta_i & \text{otherwise} \end{cases}
\end{align*}
\]

Figure 2 – (a) Actuator with rate and magnitude saturations. (b) Model used to represent such an actuator (scalar case)

The dynamical model of the actuator is based on Scheme 2(b) as follows:

\[
sysACT : \begin{cases} 
\dot{v} = v + \phi_i(v) \\
u_{cs} = T_i y_{cs} + T_0 \phi_i(y_{cs}) - T_0 v
\end{cases}
\]

where \( \phi_i(v) = \text{sat}_{\delta_i} (v) - v \), and \( \phi_i(v) = \text{sat}_{\delta_i} (v) - v \cdot \text{sat}_{\delta_i} (v) \) are classical saturation functions and \( u_{cs} \) and \( u_i \) are the levels of saturation in magnitude and rate, respectively. The elements of the diagonal matrix \( T_0 \in \mathbb{R}^{n_{cr} \times n_{cr}} \) classically take on large enough values, in order to avoid affecting the linear dynamics of the closed-loop system.

Anti-windup compensator

In the DLAW (Direct Linear Anti-Windup) strategy, the anti-windup controller uses as input the difference between the signals issued either from the input and the output of the whole actuator or from the input and the output of the nonlinear elements included in the actuator. Then, the anti-windup loop under consideration in the paper considers that the inputs of the anti-windup controller are the dead-zones associated with each saturation. Hence, the anti-windup controller of order \( n_{aw} \) is written as:

\[
\begin{align*}
\text{AW}_c : & \quad \begin{cases} 
\dot{x}_{aw} = A_{aw} x_{aw} + B_{aw} \phi_i(y) + B_{aw} \phi_i(v) \\
y_{aw} = C_{aw} x_{aw} + D_{aw} \phi_i(y) + D_{aw} \phi_i(v)
\end{cases}
\end{align*}
\]

where \( v_c \) and \( v_s \) are of dimensions \( n_{cr} \) and \( m_s \), respectively.

Interconnections

The interconnections considered can be described as follows:

- linear link between the output of the plant and the input of the controller: \( u = y_p \).
• the first part of the output of the controller \( y_c \) is linked to the corresponding inputs of the plant \( u_i \) through the actuator model (3);
• the second part of the output of the controller is directly connected to the corresponding inputs of the plant: \( u_{aw} = y_{awi} \);
• \( v_c \) and \( v_r \) are built from the anti-windup compensator.

Remark 2.1
An important fact is that the anti-windup model (4) imposes the assumption that the input and output signals of each saturation block in Figure 2 are available. To overcome this assumption, alternative strategies can be investigated. For example, the anti-windup may use the difference between the nonlinear actuator and a linear fictitious one (with the same dynamics but without saturation blocks) to explicitly take into account the dynamics of the actuator (present in the rate limiter) [20]. Another option would be to build an observer to evaluate the internal state of the actuator [27].

Standard formulation
In [24], a standard formulation of the anti-windup design has been proposed for various kinds of actuators. In the current case, by considering an augmented state of dimensions \( n = n_r + n_u + n_u + n_{aw} \), including the state of the plant, the state of the actuator, the state of the controller and the state of the anti-windup controller, the following standard model of the complete closed-loop system can be defined by:

\[
\begin{align*}
\dot{x} &= A x + B_0 (y_c) + B_1 w

\dot{y}_c &= C_0 x + D_0 (y_c) + D_1 w

\dot{v} &= C_1 x + D_1 (y_c) + D_2 w

\dot{z} &= C_2 x + D_2 (y_c) + D_3 (v + D_3 w)
\end{align*}
\]

(5)

where the matrices of the anti-windup controller are encapsulated into the matrices of system (5). Details of these matrices are given in Section “Algorithms for \( AW_g \) design”.

The design procedure of the anti-windup controller consists in optimizing some quantities, such as the size of the region of stability of the closed-loop system or the guaranteed level of performance. In particular, the idea when adding the anti-windup loop is to maximize the closed-loop system or the guaranteed level of performance. To this end, one could consider the size of the region of stability of the closed-loop system (5) or the guaranteed level of performance for the closed-loop system (5). The result considers existence conditions to solve Problem 2.2.

Main anti-windup design conditions
Solution to standard anti-windup design

The following proposition provides conditions of local stability and \( L_2 \) performance for the closed-loop system (5). The result considers existence conditions to solve Problem 2.2.

Proposition 3.1
If there exist a symmetric positive definite matrix \( Q \in \mathbb{R}^{n \times n} \), two matrices \( Z_i \in \mathbb{R}^{n \times n} \) and \( S_i \in \mathbb{R}^{n \times n} \), two positive diagonal matrices \( D \) and \( S \) and a positive scalar \( \gamma \) such that the following conditions are met:

\[
\begin{bmatrix}
Q A + A' Q - Q C_i - Z_i \n -2 S_i - D_i S_i - S_i D_i' \n -2 S_i - D_i S_i - S_i D_i' + D_i S_i D_i' \n -S_i - D_i S_i + D_i S_i D_i'
\end{bmatrix} < 0 \quad (7)
\]

then,

1. when \( w = 0 \), the set \( E \{ Q^{-1} \delta \} = \{ x \in \mathbb{R}^n ; x' Q^{-1} x \leq \delta^{-1} \} \) is RAS for the closed-loop system (5);
2. when \( x(0) = 0 \), satisfying (6), and for \( x(0) = 0 \),
   - the trajectories of the closed-loop system remain bounded in the set \( E \{ Q^{-1} \delta \} \);
   - the \( L_2 \) gain is finite and one obtains:

\[
\int_0^T x'(t) z(t) dt \leq \gamma \int_0^T w(t) w(t) dt, \forall T > 0 \quad (10)
\]

The detailed way to derive the conditions and to prove them can be found, for example, in [24], [31].

Remark 3.2
The interest of the anti-windup structure resides in the simplicity of the design conditions. Indeed, the design of a static anti-windup gain (only matrices \( D_i' \) and \( S_i' \) are used) is the result of a fully linear problem. In the case of the design of a dynamical anti-windup controller, for a priori given matrices \( A_{aw} \) and \( C_{aw} \), the determination of the input and transmission matrices is also obtained by solving a linear problem. In the case where \( n_{aw} = n_r + n_u + n_u \), the resolution of a linear problem can also be considered through an iterative procedure [24].

For analysis purposes (the anti-windup controller being given), the conditions of Proposition 3.1 are linear and can be directly used to solve adequate optimization problems. Moreover, in the design context, the conditions of Proposition 3.1 are non-convex, matrices \( A_{aw} \), \( B_{aw} \), \( C_{aw} \) and \( D_{aw} \), hidden in matrices \( A \), \( B \), \( C_{aw} \), \( D_{aw} \) \( i, j = 0,1 \). Conditions with linear decision variables can be obtained, more or less directly, by slightly modifying the original conditions, or even by considering iterative procedures (including D-K iteration process).
allowing a Lyapunov matrix and anti-windup matrices to be sought. These situations are detailed in the next subsection.

Remark 3.3
In the sequel, one considers a set $\mathcal{X}_0$, defined by some directions in the plant state space $v_i \in \mathbb{R}^n$, $i = 1, \ldots, q$, to provide a desired shape of the region $E(Q^{-1}, \delta)$ to be maximized when solving Problem 2.2. Then, considering $V = [v_0, 0] \in \mathbb{R}^n$, $i = 1, \ldots, q$ and $\beta$ a scaling factor such that $\beta v_i \in E(Q^{-1}, \delta)$, $i = 1, \ldots, q$ (which corresponds to imposing $\beta \chi_0 \subset E(Q^{-1}, \delta)$), an additional condition to those of Proposition 3.1 must be considered in the algorithms, as follows:

$$\begin{bmatrix} \frac{\delta}{\beta^2} & \delta v_i \\ \delta v_i & Q \end{bmatrix} > 0, \ i = 1, \ldots, q \quad (11)$$

This means that $\beta$ is used to maximize the region of attraction of the system and $\mathcal{X}_0$ allows the directions of interest for this region of attraction to be oriented.

### Algorithms for $AW$ design

From (1), (2), (3) and (4), the matrices of system (5) are defined by:

$$A = \begin{bmatrix} A & B_{Cw} \\ 0 & A_{sw} \end{bmatrix}, \quad B_0 = \begin{bmatrix} B_{\phi} + B_{Dw} \\ B_{sw} \end{bmatrix}, \quad B_1 = \begin{bmatrix} B_{\phi} + B_{Dw} \\ B_{sw} \end{bmatrix}$$

$$C_0 = \begin{bmatrix} C_0 & C_0C_{sw} \\ 0 & C_0 \end{bmatrix}, \quad C_1 = \begin{bmatrix} C_1 \end{bmatrix}, \quad C_2 = \begin{bmatrix} C_2 & 0 \end{bmatrix}$$

$$D_{00} = C_{sw}D_{sw}^0, \quad D_{01} = C_{sw}D_{sw}^1, \quad D_{10} = \alpha + C_{sw}D_{sw}^0, \quad D_{11} = C_{sw}D_{sw}^1$$

$$B_2 = \begin{bmatrix} B_2 \\ \end{bmatrix}, \quad D_0 = 0, \quad D_1 = 0$$

with

$$\alpha = \begin{bmatrix} A_{sw} + B_{sw}D_{sw}^{-1}D_{sw}^{\dagger}C_{sw} \\ \end{bmatrix}, \quad B_{ps} = \begin{bmatrix} B_{ps} + B_{ps}D_{ps}^{-1}D_{ps}^{\dagger} \\ B_{ps} \end{bmatrix}$$

$$C_0 = \begin{bmatrix} D_{sw}^{\dagger}(I + D_{sw}D_{sw}^{-1}D_{sw}^{\dagger})C_{sw} \\ D_{sw}^{\dagger}(I + D_{sw}D_{sw}^{-1}D_{sw}^{\dagger}) \\ \end{bmatrix}, \quad C_1 = \begin{bmatrix} C_{sw}D_{sw}^{-1}C_{sw} \\ C_{sw} \end{bmatrix}, \quad C_2 = \begin{bmatrix} C_{sw}D_{sw}^{-1}C_{sw} \\ C_{sw} \end{bmatrix}$$

$$D_{00} = D_{sw}^{\dagger} + D_{sw}^{\dagger}D_{sw} + D_{sw}^{\dagger}D_{sw}^{-1}(D_{sw}D_{sw} + D_{sw}^{\dagger})$$

$$D_{10} = T_0(D_{sw}^{\dagger}D_{sw} + D_{sw}^{\dagger}D_{sw}^{-1}(D_{sw}D_{sw} + D_{sw}^{\dagger}D_{sw} + D_{sw}^{\dagger}))$$

Furthermore, matrices defining the interconnection between the anti-windup loop and the system are:

$$B_{w} = \begin{bmatrix} 0 \\ T_0D_{sw} \end{bmatrix}, \quad C_{sw} = \begin{bmatrix} I_{sw} \\ 0 \end{bmatrix}, \quad C_{1w} = \begin{bmatrix} T_0D_{sw} \end{bmatrix}$$

$$D_{sw} = D_{sw}^{\dagger}(D_{sw}D_{sw} + D_{sw}^{\dagger})$$
The analysis problem (Algorithm 3.4) is linear and the synthesis problem of the anti-windup is nonlinear, including products between decision variables and, in particular, between the Lyapunov matrix $Q$ and the anti-windup elements. A D-K iteration procedure may then be considered for the synthesis problem (Algorithm 3.6). However, the synthesis optimization problem may be partially linearized and, for given matrices $A_{aw}$ and $C_{aw}$, the design of matrices $B_{aw}$ and $D_{aw}$, $i = 0,1$ can be handled via a linear optimization problem (Algorithm 3.5).

**Algorithm 3.4**

Analysis of a given AW$_i$ anti-windup controller

1. Select matrices $A_{aw}$ and $C_{aw}$. A static anti-windup AW$_i$ may also be used by considering $n_{aw} = 0$.
2. Choose directions to be optimized $v_j \in \mathbb{R}^r$, $i = 1,\ldots,q$ and a known perturbation bound $\delta$.
3. Solve
   \[
   \min Q, S_i, S_0, q_0, r_i, r_0, \gamma, \mu \quad f_{cost}(\gamma, \mu)
   \]
   subject to LMI (7), (8), (9) and (11)

   where $\gamma$ is the $L_2$ gain between $w$ and $z$ and $\mu = 1/\beta^2$.

**Algorithm 3.5**

Design of an AW$_i$ anti-windup controller with fixed dynamics

1. Select matrices $A_{aw}$ and $C_{aw}$. A static anti-windup AW$_i$ may also be used by considering $n_{aw} = 0$.
2. Choose directions to be optimized $v_j \in \mathbb{R}^r$, $i = 1,\ldots,q$ and a known perturbation bound $\delta$.
3. Solve
   \[
   \min Q, S_i, S_0, q_0, r_i, r_0, \gamma, \mu \quad f_{cost}(\gamma, \mu)
   \]
   subject to LMI (7), (8), (9) and (11)

   where $\gamma$ is the $L_2$ gain between $w$ and $z$ and $\mu = 1/\beta^2$.

4. Compute $B_{aw} = B_{aw}^i S_{aw}^{-1}$, $B_{aw}^i = B_{aw}^i S_{aw}^{-1}$, $D_{aw} = D_{aw}^i S_{aw}^{-1}$ and $D_{aw}^i = D_{aw}^i S_{aw}^{-1}$.

**Algorithm 3.6**

Design of an AW$_i$ anti-windup controller – full design

1. Select matrices $A_{aw}$ and $C_{aw}$ of appropriate dimensions, in order to build the desired anti-windup loop.
2. Choose the directions to be optimized $v_j \in \mathbb{R}^r$, $i = 1,\ldots,q$ and a known perturbation bound $\delta$.
3. Pre-synthesis step – Solve
   \[
   \min Q, S_i, S_0, q_0, r_i, r_0, \gamma, \mu \quad f_{cost}(\gamma, \mu)
   \]
   subject to LMI (7), (8), (9) and (11)

   where $\gamma$ is the $L_2$ gain between $w$ and $z$ and $\mu = 1/\beta^2$.

4. Compute $B_{aw} = B_{aw}^i S_{aw}^{-1}$, $B_{aw}^i = B_{aw}^i S_{aw}^{-1}$, $D_{aw} = D_{aw}^i S_{aw}^{-1}$ and $D_{aw}^i = D_{aw}^i S_{aw}^{-1}$.

5. If the solution obtained is satisfactory (some accuracy has to be fixed), or no longer improved compared to the previous steps, then STOP. Otherwise, go to the next iteration (the idea is to finish by a pre-synthesis step).

6. Synthesis step – Pick the solution $Q$ obtained at Step 3 and solve
   \[
   S_i, S_0, q_0, r_i, r_0, \gamma \quad f_{opt}(\gamma, \mu)
   \]
   subject to LMI (7), (8), (9) and (11)

7. Go to Step 3.
Actually, the current published version of the toolbox does not allow the dynamic anti-windup design problem to be formally solved in the presence of position and rate saturation, but gives many elements to extend the functions to the case addressed in this paper.

Alternatively, the AWAST Tools [5], which were recently updated and integrated as a library (SAW Library) of the SMAC Toolbox [4], enable rather general anti-windup problems to be formalized and solved, following the practical framework proposed in [6].

**PIO alleviation using an anti-windup loop**

The design and analysis algorithms of Section “Main anti-windup design conditions” are now applied and compared in the realistic context of lateral maneuvers of a civil transport aircraft. Specific attention is devoted to aggressive pilot demands in conjunction with actuator loss.

To do this, the pilot’s activity is modeled as a static gain $K_{pil}$. For this application, a normal activity would correspond to $K_{pil} = 1$. Actually, in stressful situations, notably in case of actuator loss, a more aggressive pilot behavior is generally observed, resulting in much higher gains. Here, the gain is set to $K_{pil} = 2$.

**Problem setup and objectives**

A nonlinear closed-loop Simulink implementation of the anti-windup structure is depicted in Figure 3. The “aircraft” block is a linearized version (for fixed airspeed and altitude under cruise flight conditions) of the lateral dynamics of the system, including structural filters and delays, resulting in a state-space model of dimension 63. The controller block includes a dynamical controller of dimension 29. Its central objective is to provide good damping for the Dutch roll and to enable a safe control of the roll rate so that the bank angle $\phi$ is then easily controlled by the pilot with a simple gain $K_{pil}$. The state-space models $sysP$ and $sysC$ are then readily obtained from the Simulink diagrams of Figure 3, with the help of the Matlab `linmod` function. The plant corresponds to the “yellow box” depicting the aircraft system while the global controller (including pilot actions) is obtained by extraction of the 3 blue boxes. A standard balanced reduction technique is finally applied to obtain reasonably sized models. The reduced orders obtained, respectively $n_p = 8$ and $n_c = 20$, are compatible with the proposed algorithms.

The aircraft system involves 2 control inputs ($m = 2$): ailerons and rudder deflections. Note that only the aileron deflection actuator is assumed to saturate ($m_s = 1$) for the considered maneuvers. Moreover, 5 outputs ($p = 5$) are available for feedback ($y_s = [\beta, p, r, \phi, \dot{\phi}]^T$). The performance is evaluated via the tracking accuracy on the fourth bank-angle output $\phi$ (then, $l = 1$). The disturbance input of System (1) is used to express the perturbing effect of the saturation of the system input, that is, $B_{ps}' = B_{ps}'(q = 1)$.

In the $AW$ strategy, two signals (one for the magnitude limitation and one for the rate limitation) are used by the anti-windup device. Their generation is detailed in the Simulink implementation of Figure 4.

The anti-windup controller acts on the internal dynamics of the nominal lateral controller of the aircraft through two scalar signals $v_c$ and $v_h$, which respectively affect roll and sideslip angle dynamics ($v_s = [v_r, v_h]$ and $v_s = 0$, $n_r = 2$, $n_c = 0$). This means that matrix $B_{rr}'$ appearing in Equation (2) is of dimension $n_r \times 2$.

The chosen strategy offers some flexibility, with the possibility of a direct anti-windup action at the controller output. However, no significant improvement has been observed with this additional feature, which has thus not been further considered in this application. This means that $D_{rr}'$ appearing in Equation (2) is equal to 0.
The main objective of this application is to design and evaluate anti-windup compensators to improve the aircraft response to roll angle solicitations while limiting oscillations despite actuator loss [18]. During such maneuvers, a significant control activity is observed on the ailerons. This is why the effects of saturations are modeled and taken into account for these actuators in the diagram of Figure 3, while no saturation is introduced on the rudders. The effects of saturations become even more penalizing in case of a partial loss of control capability. Assume indeed that the aircraft is controlled by a pair of ailerons on each wing, but that only one is operational. In that case, the activity of the remaining actuators is doubled, as well as the risk of magnitude and rate saturations. Then, the magnitude and rate limits in the following are halved. We consider \( u_0 = L_m = 10 \) deg (instead of 20 under normal conditions) and \( u_1 = L_r = 20 \) deg (instead of 40).

In the following, various cases studies are implemented and compared:

- Unsaturated – A non-saturated case where saturation elements are removed allows an ideal behavior of the closed-loop system to be exhibited;
- Saturated – A saturated case without compensation strategy is used as the nominal behavior of the closed-loop saturated system;
- Anti-PIO filter – The standard anti-PIO filter used in the industry consists in adding a dynamical block with pre-saturation before the rudder input. Thus, the anti-windup action significantly improves the transient behavior of the roll angle, avoiding a large overshoot and degraded time evolution of construction for engineers who are not always specialists in advanced control theories. Note that, unlike the approach addressed in this paper, the signal used as input for the anti-windup scheme is the difference between the output and the input of the nonlinear block (denoted by \( e \)).

In what follows, reduced size models are used for stability analysis and to compute the anti-windup controllers. Full size models of the aircraft and controllers are used for all of the simulations.

### Design of a static anti-windup \( AW \)φ

Let us first consider the design of a static \( AW \)φ anti-windup where only matrices \( D_{aw} \), \( i = 0, 1 \) (see Equation (4)), have to be designed (\( n_m = 0 \)). The main advantage is that Condition (7) becomes linear and that the anti-windup block does not involve any additional dynamics. The optimization problem is solved by considering the bound on perturbation \( \delta = 0.1 \) and \( v_1 = [C_e(4:0)] \), corresponding to the roll angle, as the direction to be optimized over the set \( E(Q^{-1}, \delta) \). Algorithm 3.5, followed by Algorithm 3.4, provide the following optimal solution:

**Static \( AW \)φ design:** \( \gamma = 1.18110; \beta = 0.7808 \)

with the static anti-windup gains:

\[
D^0_{aw} = \begin{bmatrix} -14.7887 \\ 8.6544 \\ 0 \end{bmatrix}, \quad D^1_{aw} = \begin{bmatrix} -0.0042 \\ 0.0392 \\ 0 \end{bmatrix}
\]

which shows that the anti-windup hardly uses the rate saturation information. Moreover, it is interesting to perform the same analysis for the saturated closed-loop system without anti-windup. The feasibility is also obtained and the solution is:

**Analysis without anti-windup:** \( \gamma = 1.8560; \beta = 0.7796 \)

The solution with the static \( AW \)φ anti-windup described through \( \gamma \) and \( \beta \) as performance indicators does not appear to be much better than the one without anti-windup: the anti-windup allows \( \gamma \) to be decreased and \( \beta \) to be increased, but only slightly. This does not reflect, however, the simulations described below, which show that the anti-windup action significantly improves the transient behavior of the roll angle, avoiding a large overshoot and degraded time evolution.
with respect to the saturated case. The meaning of this is that the considered optimization criterion, which does not explicitly include the time response performance, does not exactly fit the analysis or design of the anti-windup loop. Nevertheless, considering criteria on time response performance is a difficult task and the optimization criterion used here gives a reasonable trade-off between stability guarantee, performance and time response.

Figures 5 and 6 illustrate the time evolution of the closed-loop system to a roll solicitation of 40 deg at time $t = 1$ s followed by a step of −60 deg at time $t = 15$ s and a step of +60 deg at time $t = 30$ s. The responses are compared by considering the case with saturation and no compensation (saturated), a standard anti-PIO strategy (anti-PIO filter) and the static $AW_s$ anti-windup strategy. It is important to underline that a simple static anti-windup strategy enables better performance than the standard anti-PIO case to be obtained, which adds dynamics to the system.

**Design of a dynamic anti-windup $AW_d$**

To go further, let us now consider the design of a dynamic anti-windup $AW_d$. The difficulty in this case is to initialize the iterative procedure described in Algorithm 3.6, or to select matrices $A_{aw}$ and $C_{aw}$ used in Algorithm 3.5. As for the static case, the optimization problem is solved by considering the bound on perturbation $\delta = 0.1$ and $v_i = [C_p(\psi_i) \theta]$ as the direction to be optimized over the set $\varepsilon(Q^\infty, \delta)$.

Let us first consider a very simple structure to set matrices $A_{aw}$ and $C_{aw}$, namely a modal structure for $A_{aw}$, allowing its dynamics to be set slightly faster than those of the closed-loop linear system:

$$A_{aw} = \begin{bmatrix} -100 & 50 \\ -50 & -100 \end{bmatrix}, \quad C_{aw} = \begin{bmatrix} -10 & 0 \\ 0 & 10 \end{bmatrix}$$

Algorithm 3.5 followed by Algorithm 3.4 provides the following optimal solution:

**Dynamic $AW_d$ design 1:** $\gamma = 1.7863; \beta = 0.8334$

with the anti-windup terms:

$$B_{aw}^0 = \begin{bmatrix} 9461.4 \\ -7872.5 \end{bmatrix}, \quad B_{aw}^1 = \begin{bmatrix} 60.6 \\ -32.9 \end{bmatrix}, \quad D_{aw}^0 = \begin{bmatrix} 438.2 \\ 1009 \end{bmatrix}, \quad D_{aw}^1 = \begin{bmatrix} 3.5 \\ 0 \end{bmatrix}$$

Another option is to use matrices $A_{aw}$ and $C_{aw}$, which are the solution to another dynamic anti-windup scheme implemented on the same application. The idea is to circumvent the nonlinear problem of the dynamic anti-windup by pre-selecting matrices $A_{aw}$ and $C_{aw}$ obtained from other approaches, when they exist, with the expectation of obtaining better results than with a “random” selection as done above. In the current case, we consider the solution obtained with a structured $\mathcal{H}_\infty$ design method [18], and previously applied on the same numerical evaluation [7]. In that case, Algorithm 3.5 gives matrices $B_{aw}'$ and $D_{aw}'$, $i = 0.1$, (not provided here for readability reasons) and the following optimal solution:

**Dynamical $AW_d$ design 2:** $\gamma = 1.7395; \beta = 0.9147
A roll solicitation of 40 deg at time \( t = 1 \) s followed by a step of
–60 deg at time \( t = 15 \) s and a step of +60 deg at time \( t = 30 \) s
is considered to compare the results. The time responses of the roll
angle for the case without saturation, with the \( \mathcal{H}_\infty AW \) anti-windup
resulting from [7] and the designed dynamic \( AW \) anti-windups are
plotted in Figure 7. Similarly, the time evolutions of the control input
\( \delta_c \) in these cases are depicted in Figure 8.

One can observe that the level of performance of the very well-tuned
\( \mathcal{H}_\infty AW \) anti-windup is slightly degraded in comparison with the two
cases of \( AW \) design, but it remains acceptable and close to the ideal
response that would be obtained if no saturation was present in the
actuator block. One can also remark that the dynamic anti-windup
design makes it possible to speed-up the rising time (less than 6
seconds) toward the set-point, with respect to the static anti-windup
design (more than 6 seconds), even with very basic anti-windup
dynamics (\( AW \) design 1).

**Complementary illustrations**

The rate-saturation effectiveness is illustrated in Figures 9 and 10,
where the signals \( v \) and \( x_c \) are plotted, respectively, for the case with
and without anti-windup. One can check that the anti-windup action
both reduces the number of rate-saturation events and the amplitude
of the signal \( v \) entering the saturation element (see Equation (3)).

Moreover, the stick response of the system, i.e., the output of the
pilot gain block, is plotted in Figure 11 to illustrate the efficiency of
the anti-windup design. In this case, with a moderately aggressive
pilot (\( K_{pol} = 2 \)), one can check that the pilot workload increases in
is set to 5 s to generate sufficient excitation in the aircraft modes of motion.

This illustrates the situation where strong excitation of the lateral aircraft modes of motion may result in the instability of the saturation response. Anti-PIO and anti-windup strategies allow stability to be preserved. Moreover, the dynamic anti-windup strategy enables a good tracking of the reference to be preserved, when the standard anti-PIO and the static anti-windup induce degraded responses with overshoot even if stable.

**Conclusion**

An anti-windup design strategy has been proposed for systems involving both magnitude and rate saturations, and taking into consideration that such saturations elements only affect some of the inputs. Such a situation is illustrated on a lateral flying model of a civil aircraft undergoing moderately aggressive maneuvering by the pilot. For this kind of systems, it is well known that magnitude and rate saturations of the aileron deflection actuator may lead to an undesirable behavior, often called Pilot-Induced-Oscillation (PIO). Anti-windup compensators have been designed through adequate convex optimization schemes, and a comparison with given dynamic anti-PIO filters already developed has also been provided. The numerical evaluation has made it possible to show, first, that a static strategy provides better results than classical anti-PIO filters basically used in industry. Moreover, the increase in the complexity of dynamic anti-windup compensators (both in terms of structure and computation) is compensated by the fact that they make it possible to recover behaviors very close to that which would be obtained if the actuators were linear. In any case, there is room for future work, such as the design of other anti-windup schemes, which may include the parameter-varying approach [21] or reset controllers [25].
Acronyms

AW (Anti-Windup)
DLAW (Direct Linear Anti-Windup)
LMI (Linear Matrix Inequality)
MRAW (Model Recovery Anti-Windup)
PIO (Pilot-Induced-Oscillation)

References

[18] G. PUYOU, J.-M. BIANNIC - Application of Robust Antiwindup Design to the Longitudinal Aircraft Control to Cover Actuator Loss. 19th IFAC Symposium on Automatic Control, University of Wurzburg, Germany, September 2013.
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